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System performance of a cryogenic test-bed for the time-division multiplexing readout for the NewAthena X-ray Integral Field Unit

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ABSTRACT. The X-ray Integral Field Unit (X-IFU) is an instrument of European Space Agency's future NewAthena space observatory, with the goal to provide high-energy resolution (<4 eV at X-ray energies up to 7 keV) and high-spatial resolution (9 in.) spectroscopic imaging over the X-ray energy range from 200 eV to 12 keV, by means of an array of ~ 1500 transition-edge sensors (TESs) read out via superconducting quantum interference device time-division multiplexing (TDM). A TDM-based laboratory test bed has been assembled at Netherlands Institute for Space Research, hosting an array of $75 \times 75 \mu\text{m}^2$ TESs that are read out via 2-column $\times$ 32-row TDM. A system component that is critical to high-performance operation is the wiring harness that connects the room-temperature electronics to the cryogenic readout componentry. We report here on our characterization of such a test bed, whose harness has a length close to what was envisioned for X-IFU, which allowed us to achieve a co-added energy resolution at a level of 2.7-eV full width half maximum at 6 keV via 32-row readout. In addition, we provide an outlook on the integration of TDM readout into the X-IFU focal plane assembly development model.

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1 Introduction

Advanced Telescope for High-Energy Astrophysics (NewATHENA) is European Space Agency's next X-ray astronomical observatory that will study the hot and energetic universe¹ from an L1

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Sun–Earth orbit, with a launch foreseen for 2037. On board the satellite, there will be two instruments: the Wide-Field Imager designed for imaging surveys in a $40' \times 40'$ field of view and 0.2- to 15-keV band with DEPFET pixels, and the X-ray Integral Field Unit² (X-IFU) optimized for imaging spectroscopy.

The X-IFU will make use of ≈ 1500 transition-edge sensors (TESs) micro-calorimeters,³ organized in a hexagonal array covering a field of view of $4'$ with a pixel size of $317 \mu\text{m}$ corresponding to $5''$ point spread function angular resolution. The sensors will be cooled down to a base temperature of 50 mK by means of a multi-stage adiabatic demagnetization refrigerator (ADR) and are designed to operate in the soft X-ray energy band, between 200 eV and 12 keV, with a predicted energy resolution at instrument level better than 4 eV for energies up to 7 keV.

To comply with the stringent requirements of mass, volume, and heat load for the cryogenic stages of the instrument, a multiplexing readout scheme is necessary. Time-division multiplexing (TDM)⁴ has been selected, as it is a mature technology routinely used in ground-based X-ray and γ -ray spectrometers, such as the Stanford Synchrotron Radiation Lightsource beamlines at Stanford Linear Accelerator Center (United States) and recently in the Micro-X sounding rocket.⁵

In TDM readout, the TESs are continuously dc-biased and are each coupled to a first-stage SQUID (SQ1), activated one at a time via a flux-actuated switch (FAS). SQ1 signals are amplified by a superconducting quantum interference device (SQUID) series array (SSA) and digitized by room-temperature electronics. Each SQ1 represents a “row,” and the FASs are activated by sequential square wave signals, or row-addressing signals (RAS), generated by the digital readout electronics (DRE). The SQ1s are hosted on “MUX” chips, together with the shunt resistance R_{sh} to voltage bias the TES and Nyquist inductors L_{Ny} to limit the pixel bandwidth. Each row is active for a certain “row time,” all the N rows are read out within one “frame” and the M columns are read out in parallel. An explicative depiction of the operation of a TDM readout for micro-calorimeters can be found in Fig. 8 of the recently published review “Signal Readout for Transition-Edge Sensor X-ray Imaging Spectrometers.”⁴ For X-IFU, a 48-row $\times$ 32-column TDM readout is envisaged, with row time of 160 ns.

Netherlands Institute for Space Research (SRON) is responsible for the design, development, and delivery of X-IFU’s focal plane assembly (FPA). The first iteration of the FPA development model (FPA-DM) was employing a TES array⁶ and a frequency-domain multiplexing (FDM)⁷ technology, both developed at SRON. It was successfully used to validate its thermo-mechanical and magnetic environment. A second iteration of the FPA-DM, called DM1.1,⁸ is foreseen before upscaling to the FPA engineering model, which will employ a TDM architecture. For the assembly and test campaign of the DM1.1, expected to start in Q2 2025, SRON will receive key components from several external partners: the TES array and the digital room-temperature electronics (DRE) from NASA-GSFC (United States), the MUX chips from National Institute for Standards and Technology (NIST, United States), and the warm front-end electronics from APC-CNRS (France).

In late 2022, our team assembled components from SRON, NIST, and NASA-GSFC into a new cryogenic test bed at SRON, as described in Sec. 2. The motivation was to transfer TDM technology from the development laboratory to a more flight-like configuration ahead of its implementation in the DM1.1. Driven by the NewAthena spacecraft geometry, the flight-like TDM system will require a significantly longer wiring harness, linking the room-temperature electronics to the cryogenic componentry, than what is typically used in laboratory TDM systems.

Such a harness is critical for several aspects of the system operation, including crosstalk, low-frequency signal transfer from the SSA SQUID to the low-noise amplifier (LNA) at the room temperature electronics, the noise contribution of the harness resistance, and the open-loop bandwidth of the signal transfer. Parameters such as harness length and termination on both the cold and the warm part of the readout have an impact on the aforementioned aspects of the system.

This new test bed at SRON uses a longer wiring harness than laboratory TDM systems. An upgrade in late 2023 introduced a re-designed version of the long harness (see Sec. 2.1). Our main recent goal was to reproduce in this new system the nominal spectral performance of the previous laboratory systems: 2.8 eV full width half maximum (FWHM) or better energy resolution at 6 keV under two-column $\times$ 32-row multiplexing.

In this paper, we report on the experimental activities performed with such a cryogenic test bed at SRON. In Sec. 2, we describe both the hardware and software composing the experimental

setup. In Sec. 3, we describe the characterization tests performed to optimize and debug the system. In Sec. 4, we show the performance demonstration, in agreement with the nominal specifications. Finally, in Sec. 5, we summarize our results and give a prospect for future activities.

2 Description of the Setup

For ease of reading, we subdivide the components of the test bed into three categories: cryogenic assembly, room-temperature electronics, and control software.

2.1 Cryogenic Assembly

The cryogenic assembly is mounted in a Leiden Cryogenics dilution refrigerator (model CF-CS81-400), having a nominal cooling power of $400 \mu\text{W}$ at 120 mK. The typical base temperature of the mixing chamber during full-load operation, with multiple X-ray TES microcalorimeter experiments assembled in the refrigerator, is 18 mK. The TDM system is depicted in Fig. 1, and it consists of the following components.

2.1.1 50-mK snout

A “50-mK snout”⁹ hosts the TES¹⁰ and MUX chips¹¹ [Fig. 1(a)]. The detector array, provided by NASA-GSFC, is a kilo-pixel chip with each TES made of $75 \times 75 \mu\text{m}^2$ Mo/Au bilayer and Bi/Au absorber, with $R_N = 9.55 \text{ m}\Omega$, $C = 1.1 \text{ pJ/K}$ at 100 mK, $G = 84.7 \text{ pW/K}$ at T_C , and $T_C = 92.5 \text{ mK}$. The MUX chips, manufactured at NIST, are of design “mux20a,”¹² in which each SQ1 is a two-SQUID series array. Accompanying “interface” chips, which contain the circuit elements for the TES-bias loop, are designed with $L_{Ny} = 640 \text{ nH}$ and $R_{sh} = 69 \mu\Omega$.

Both the TES array and MUX chips are different from the baseline design for X-IFU and are not optimized for the X-IFU level of performance, with an average single-pixel energy resolution

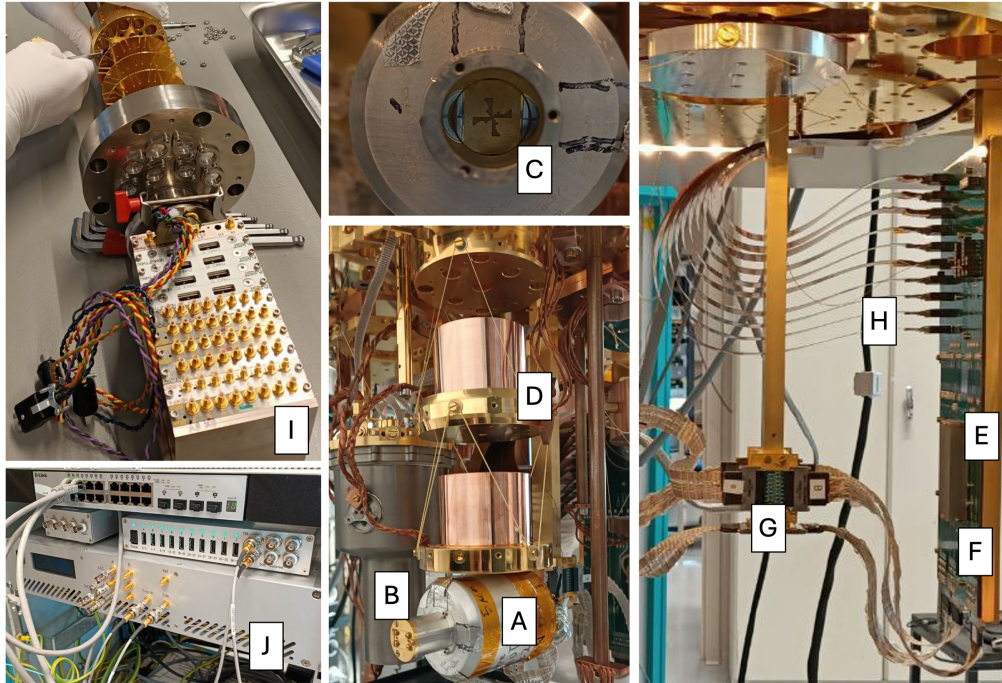


Fig. 1 Cryogenic components of the setup installed in the dilution refrigerator: 50 mK snout in Al superconducting shield (A), Fe-55 X-ray source mounted on an Al chimney in front of the TES array (B), Cu aperture mask placed in between the TES array and the X-ray source (C), two-stage Kevlar suspension system (D), 4 K board (E), SSA SQUIDs (F), inter-thermal stage boards (G) for the NbTi braided looms connecting to the 4 K to the 50 mK snout, flex harness (H), Tower (I) during system assembly, DRE (J) mounted in an electronics rack.

of ≈ 2.4 eV at 6 keV; nevertheless, these components are sufficient to allow for the technological transfer activity mentioned in Sec. 1.

The chips are enclosed in an aluminum casing to shield the TES and MUX chips from the influence of external magnetic fields. A Fe-55 radioactive source is mounted on a chimney on the aluminum casing in front of the TES array [Fig. 1(b)], to illuminate the detectors with photons of 6 keV energy, exploiting the MnK α spectral complex, used to characterize their energy resolution. A copper aperture mask [Fig. 1(c)] is placed between the TES array and the X-ray source, so that only the detectors connected to the readout are able to see the photons, to minimize thermal disturbances.

A magnetic field offset can be locally applied to the TES array by means of a superconducting coil placed directly below the detector chip.

The snout is suspended from the mixing chamber of the refrigerator using a two-stage Kevlar vibration isolation system¹³ [Fig. 1(d)] to prevent power dissipation in the TES array due to mechanical contributions in the system and mitigate low-frequency contributions to the detectors' noise from such sources, such as the pulse tube. Thermal anchoring to the mixing chamber is performed via oxygen-free high-conductivity copper braids. Temperature is monitored via a ruthenium oxide thermometer and controlled via a proportional–integral–derivative loop through a 750 Ω heater installed on the snout's mechanical support. An operating temperature of 50 mK is set, and the typical root mean square temperature stability achieved is at the level of 1 μ K.

2.1.2 4 K board and inter-stage harness

The “4 K board” [Fig. 1(e)] hosts the SA20a SSA, i.e., the second-stage amplifiers for the TES signals. Both the SSA and board assembly have been manufactured at NIST. The SSA chip is mounted within the casing for magnetic shielding [Fig. 1(f)], made of an external layer of niobium and an internal layer of cryogenic mu-metal.¹⁴ The purpose of this board is as well to provide signal routing and filtering. A number of utility connections are also available, e.g., for control of the superconducting magnet coil.

The board is mounted on a gold-plated copper mechanical support located below the mixing chamber, thermalized to the refrigerator's 3 K plate via a copper rod passing through sequential clearshots in the refrigerator's still and heat exchanger plates. A Kevlar support structure is devised on top of the mixing chamber to dampen the mechanical vibrations of the board, given the weight of its mechanical support structure and the length of the rod.

This structure is motivated by the necessity to limit the physical distance between the SSA and the MUX chips, to allow for sufficient interstage bandwidth between the two SQUID amplification stages, with the cutoff frequency $f_{3\text{ dB, interstage}}$ given by $R_{\text{dyn, SQ1}} / (L_{\text{in, SSA}} + L_{\text{stray}})$, where $L_{\text{in, SSA}}$ is the input inductance of the SSA, $R_{\text{dyn, SQ1}}$ is the dynamic output resistance of the SQ1 (or MUX SQUID), and L_{stray} is the inductive contributions coming from the 50 mK to 3 K harness, printed circuit board striplines, bonding wires, etc. Given the general requirement $f_{3\text{ dB, interstage}} \geq 12$ MHz (for a row time of 160 ns) and typical values of $L_{\text{in, SSA}} \approx 100$ nH and $R_{\text{dyn, SQ1}} \approx 15$ Ω , practical implementations require such harness length to be at a level of 30 cm. In this test bed, such a harness is constituted by niobium-titanium twisted pair looms, with a thermal break in between via inter-stage filter cards [Fig. 1(g)] thermally anchored to the heat exchanger plate (≈ 50 mK).

2.1.3 Flex harness

The connection between the “4 K board” and the warm analog electronics (“Tower,” see Sec. 2.2) is performed via the flex harness [Fig. 1(h)]. There are a total of 10 flexes, each constituted by eight supply and return conductor pairs, as diagrammed in Fig. 2. The flexes are stacked and thermalized via dedicated heatsink plates at 3 and 50 K. The interface of the flexes with the Tower electronics is described in Sec. 2.2.

The flex harness used for the measurements reported in this paper differs from the one from our previous report.¹⁵ Hereinafter, we refer to the previous design as “old flex” and the current design as “current flex”. Figure 2 shows cross-sectional diagrams to illustrate the differences between the two designs.

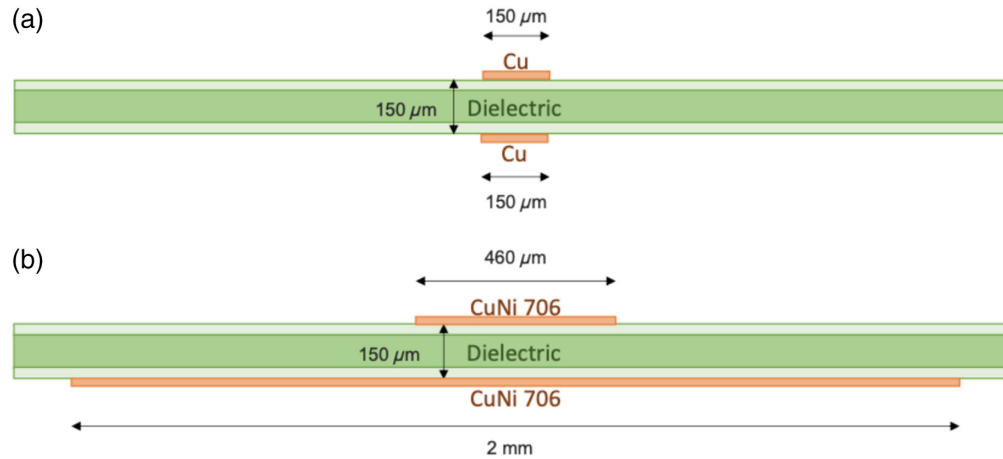


Fig. 2 Cross-section of the flex harness, comparing between the old (a) and the current (b) flex design. (a) Old flex design, used in the 16-row performance demo previously reported.¹⁵ (b) Current flex design, used in the 32-row measurement presented in this paper. The direction of current flow along the conductors is into and out of the plane of the paper. The pair pitch between adjacent wire pairs (not shown here) is 2.54 mm. The differences stand in the conductor material, symmetry between supply and return line and their individual width.

For both designs, the flex length is at a level of 1.5 m, significantly longer than the standard ≈ 40 cm used in ground-based TDM systems. The motivation for this difference was the reproduction of the nominal performance of a TDM system in an SRON dilution refrigerator, where the distance between the 3 K stage and room temperature is larger than in the ADRs available at NIST and NASA-GSFC. In addition, this is seen as an intermediate characterization of the system with a harness length closer to the 2.3 m required for X-IFU.

The old flex design employs symmetrical supply and return conductor pairs, constituted by $150\ \mu\text{m}$ Cu lines with 2.54-mm pair pitch. The dimensioning of the signal and return lines for the old flex design [Fig. 2(a)] was chosen to keep the electrical resistance below $20\ \Omega$ to be compliant with the requirements for the electronics, as well as limiting the capacitance between signal and return lines to prevent bandwidth loss. This however resulted in a larger cable inductance which enhanced electrical crosstalk in the system, inducing large electrical oscillations (“ringing”) with large amplitude, ultimately affecting the system performance already in first validation tests at NIST.

This led to the new design of the signal and return lines [Fig. 2(b)], similar to the standard dimensioning for the 40-cm length. In this case, two CuNi 706 conductor tracks are asymmetrical, with a $460\text{-}\mu\text{m}$ -wide supply line and a 2-mm-wide return line, still with a 2.54-mm pair pitch. Warm bench test measurements done at NIST showed that the level of electrical crosstalk in the harness was reduced by a factor of 20, which significantly reduced the amplitude of the ringing observed in the old flex. The wider signal track resulted however in a larger capacitance, which caused a reduction in harness bandwidth. The consequence of this is discussed in Sec. 3.

2.2 Room-Temperature Electronics

2.2.1 Analog front-end electronics

The first stage of warm electronics is represented by the “Tower”¹⁴ [Fig. 1(i)] developed at NIST. The Tower is an ensemble of modular boards each assigned to a specific function: the amplification of the signal coming from the SSA via an LNA¹⁶ and transmission to the analog-digital converter (ADC) input of the DRE, the biasing via DAC circuitry to the quiescence operating point of TES, SQ1 and SSA, connection to the feedback circuits for the SSA (flux offset) and SQ1 [flux-locked loop (FLL)], and routing of the RAS coming from the DRE.

The control of the bias boards is performed via a serial protocol, executed from the measurement computer via an optical fiber connection, whereas the connections from the Tower to the DRE are via high-bandwidth HDMI cables for the RAS and BNC cables for the ADC and feedback signals.

2.2.2 Digital readout electronics

The DRE¹⁷ is developed at NASA-GSFC and is composed of two elements: the column box and the row box [Fig. 1(j)]. The row box generates the RAS to subsequently activate the rows of each column. Synchronicity between each row's activation window (row time) and ADC sampling performed by the column box is ensured via several clocks (frame clock and line clock) generated from a master clock at 245.76 MHz. The column box furthermore handles the digital feedback for the FLL as well as the data acquisition back-end for data streaming.

2.3 Control Software

Both the DRE from NASA-GSFC and the Tower from NIST have their own custom software package for measurement and control. The Tower software is used to provide bias to the SSA and SQ1 SQUIDS and to the TES array, whereas the DRE software handles all the TDM control aspects, including row-timing and FLL settings, as well as measurement settings.

Both software are based on a graphical user interface that allows control and monitoring of the readout parameters, as well as data logging for X-ray data acquisition. To allow for automation, in view of the X-IFU FPA-DM1.1 test campaign, a dedicated control software has been developed at SRON.

This “TES-TDM Readout Software” is built on SRON's generic ground support software platform. It is designed to be scalable to a high number of readout channels, with components that require high performance implemented in C++. In addition to automated measurement scripts, a text-based user interface is provided.

3 System Characterization

3.1 Electromagnetic Interference Optimization

To prevent ground loops, a so-called star grounding scheme is used, where the top of the cryostat is used as a ground reference. All measurement electronics are grounded via thick copper braids to such reference. Electronic modules, including the column and row boxes, are powered on via an isolation transformer to decouple the ground reference of the TDM to the ground of the wall socket. Dedicated wall sockets in the laboratory, connected to separated electrical units in the building, are used for powering the readout electronics of cryogenic setups. The top of the cryostat is then connected to a “clean” ground reference in the laboratory via a thick copper grounding cable. Furthermore, to electrically decouple the connections from the Tower and the column box to the measurement computer, optical fibers are used.

Despite these precautions, strong noise lines at 50 Hz and higher harmonics have been initially observed in SQUID noise measurements. This was identified as due to electromagnetic interference (EMI) in the loop constituted by the ~3 m HDMI and BNC cables connecting the DRE to the Tower. In fact, it was observed that bundling and intertwining the cables together, to minimize the area of the loop and reject common-mode noise, significantly reduced the amplitude of such noise lines. Finally, enclosing the cable bundle in aluminum foil almost completely removed the 50-Hz noise lines. High-frequency (several kHz) lines, thought to be spurs from the DRE, remained present in the system. However, their frequency is sufficiently higher with respect to the ≈ 250 Hz of the detector's electrical bandwidth at the quiescence operating point to consider their impact negligible.

3.2 Magnetic Field Offset

As is customary for TES X-ray micro-calorimeter setups, to achieve the optimal spectral performance from the system, the behavior of the detectors under an external magnetic field has to be characterized. This is because the TES critical current is magnetic field dependent, as the system formed by the TES bilayer and the niobium leads constitutes an SS'S Josephson junction. It is typically observed that the best operation is obtained when no magnetic fields perpendicular to the bilayer are present.

These fields might be caused by external sources such as pulse tubes, Earth magnetic field, and EMI from laboratory equipment. Furthermore, TESs under dc-bias suffer from the effects of self-field, i.e., the magnetic field generated by the loop made by the leads and the TES itself.¹⁸

Such magnetic field adds to the residual field at the TES array and is bias point-dependent. The external magnetic fields are typically compensated with a superconducting coil mounted just below the TES array, as also envisaged for X-IFU.

The operating assumption is that the best spectral performance is achieved when an external magnetic field equal to the residual field without self-field is applied. To estimate this value, curves of I_{TES} versus V_{TES} at different magnetic fields B_{ext} are measured to extract how the calibrated TES current I_{TES} changes as a function of applied field for a given bias point. We then obtain I_{TES} versus B_{ext} curves, from which the well-known Fraunhofer-like trend can be extracted. The peak of such a curve for different bias points can be used to extrapolate the canceling field corresponding to when no current is flowing through the TES. A more detailed description of this method can be found in our previous report.¹⁵

As a sanity check, we also estimated the optimal canceling field with an alternative method, raising the bath temperature just below T_C and measuring the $I(B)$ curve with the minimum bias voltage to bring the TES in transition. In this configuration, I_{TES} is low and the self-field can be considered negligible so that the peak of the measured Fraunhofer pattern can be assumed to be purely due to the residual magnetic field. An example of this measurement is reported in Fig. 3.

We found the average of the canceling fields measured with both methods to be consistent. We measured an average canceling magnetic field at a level of 150 nT with no evident gradient across the array, with a few TESs showing a variation in the residual field with respect to neighboring pixels (see Fig. 4). The reason for this variation is not identified, but it could be due to either uncertainty in the measurement or a real effect in the TES array due to non-perfect uniformity. For reference, this value is nevertheless within the $\Delta B < 1 \mu\text{T}$ requirement for X-IFU for magnetic-field gradient across the TES array. Furthermore, this value of the average residual field is comparable with that typically measured for other TES setups read out under FDM hosted in the same cryostat.⁷ The minimization of magnetic field gradients is important for flight operation because TES pixels within a TDM readout column will share their dc-voltage bias and thus cannot be tuned individually to compensate for eventual different magnetic-field offsets.

3.3 Bandwidth Optimization

As mentioned in Sec. 1, the old flex design resulted in a large parasitic inductance which caused underdamped oscillations (“ringing”) in the electrical signals of the systems. Such ringing is expected to be initiated by two mechanisms: the switching transients sequentially activating the TDM rows and large changes in the feedback signal, such as when the readout switches to/from a row reading out a TES hit by an X-ray.

This mechanism can be characterized by injecting to the feedback coil of one SQ1 (first-stage SQUID) a signal of amplitude comparable to the one caused by an X-ray releasing energy in the TES. For this system, the pulse height for a 6-keV photon roughly corresponds to a signal of $2\Phi_0$, with $\Phi_0 \approx 2.067 \cdot 10^{-15} \text{ Wb}$ being the magnetic flux quantum and representing a single period in the I_{SQ1} versus Φ_{SQ1} characteristic curve.

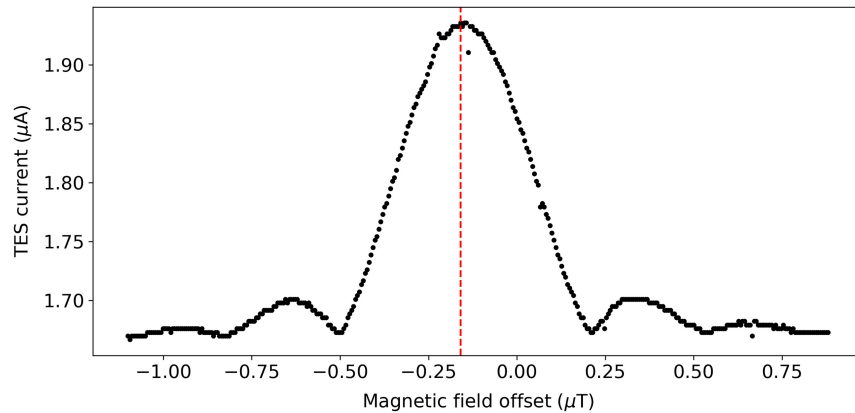


Fig. 3 Example of an I_{TES} versus B curve measured at a fixed temperature, close to T_C . The optimal magnetic field offset (red dashed line) is estimated from the peak of the Fraunhofer pattern, where I_{TES} is maximum.

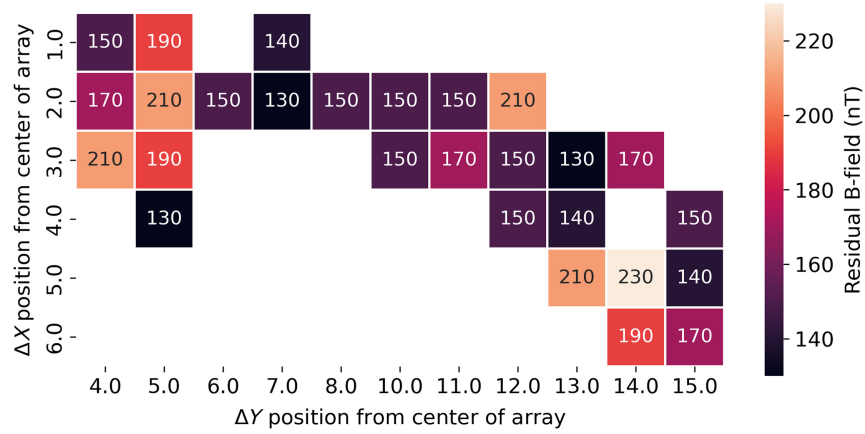


Fig. 4 Map of the canceling magnetic field measured in the TES array for one TDM column. The axis labels represent the distance on the TES array plane in pixel number units.

This experiment was performed first for the old flex and the observed response is plotted in blue in Fig. 5. We measured a peak amplitude in such oscillation at a frequency of ≈ 8 MHz, well within the system bandwidth. In TDM systems with a regular short harness, such ringing is present but at a higher frequency that is outside the typical 12 to 15 MHz readout bandwidth, allowing for 160-ns row time readout.

With the old flex harness, the system performance could be retained by operating with an increased row time of 360 ns, corresponding to a line rate of ≈ 2.7 MHz and sampling for 64 ns instead of 32 ns. As a consequence, to maintain roughly the same frame time, the multiplexing factor was reduced from 32 to 16. With this configuration, both at NIST and at SRON, similar systems were able to achieve an average energy resolution of 2.8 eV FWHM.¹⁵

Subsequently, the new flex design was implemented in the system. A ringing characterization measurement was repeated, by injecting a $2\Phi_0$ signal at the SQ1 feedback coil. In this case (Fig. 5, dashed orange curve), no underdamped oscillations were observed. However, most likely due to the larger capacitance to ground in the new design, a significantly reduced bandwidth was observed, at the level of ≈ 5 MHz.

As a consequence of this, the decay time of the transient was at a level of 200 ns, longer than the 160-ns row time, which made the use of the nominal timing settings infeasible. This effect on the switching transient due to finite analog bandwidth is known and consistent with what is reported in Durkin et al.,¹⁹ and it is equivalent to applying an aliasing filter to the SQ1 feedback signal path.

We further verified this by simulating the system behavior in a Dymola²⁰ model. A low-pass filter was inserted in the feedback path to simulate the limited bandwidth of the flexes, and the

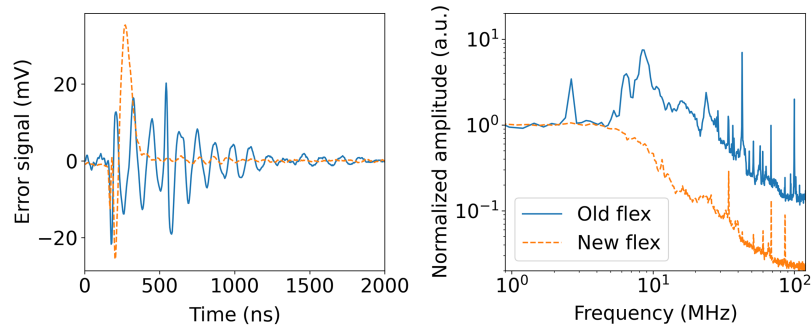


Fig. 5 Signal measured at the ADC input after injecting a $2\Phi_0$ step function at one SQ1 feedback coil. For reference, the full modulation depth of a combined SQ1/SSA SQUID curve is typically at a level of 200 mVpp. The old flex design (blue) resulted in a “ringing” with an extended settling time, whereas the new flex design (dashed orange) resulted in a transient with large amplitude and short decay time.

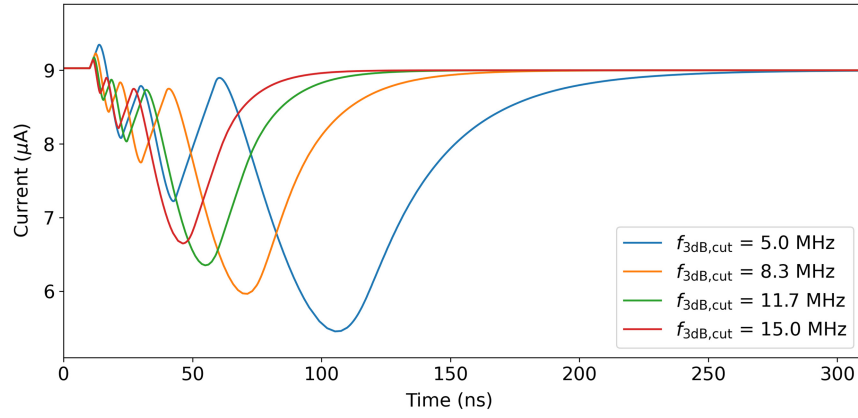


Fig. 6 Simulated signal at the input of the ADC as a function of a cutoff frequency in the SQ1 feedback path. The simulation is performed using a SQUID look-up table model in the Dymola, with a $3\Phi_0$ step function at the feedback of a single SQ1 in FLL and no input signal at the TES. Assessment method reprised from Durkin et al.¹⁹

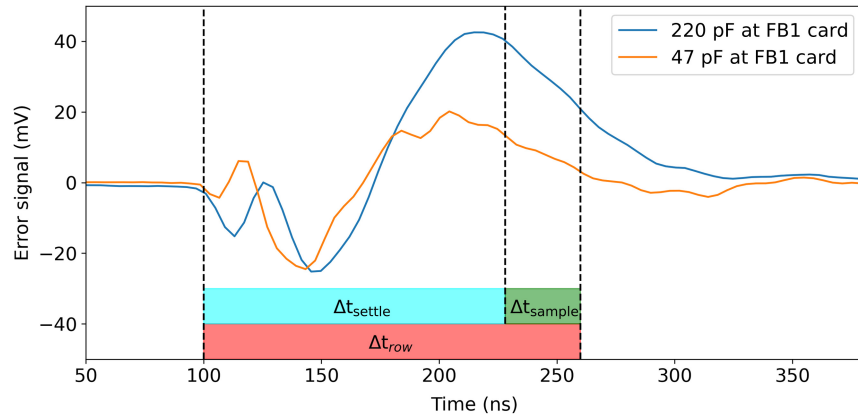


Fig. 7 Comparison of the switching transient obtained with a $2\Phi_0$ signal injected at the SQ1 feedback coil (FB1), before (220 pF) and after (47 pF) the modification to the Tower card. For 160-ns row time, the 32-ns sampling window falls within the tail of the transient in both cases; however, with the 47-pF capacitor, it is sufficiently stable and close to the baseline value to allow for 32-row operation. Assessment method reprised from Durkin et al.¹⁹

f_{3dB} cutoff was varied to several values. The impact on the transients is reported in Fig. 6, from which a cutoff at a level of 5 MHz is qualitatively consistent with the experimental observations.

To mitigate this effect, we modified the analog feedback circuitry in the Tower, increasing the cutoff of the RC bandpass filter by modifying the value of the capacitor to ground from 220 to 47 pF. The impact on the system is reported in Fig. 7. In this case, we did observe an increase in bandwidth, at a level of 7 MHz. The amplitude of the transient decreased by a factor 2, and the decay time reduced to less than 160 ns of the required row time. We considered this feasible for practical operation, re-tuning the configuration for settling time Δt_{settle} and sampling time Δt_{sample} as described in the caption of the figure. This configuration was then used to carry out the X-ray performance measurements described in Sec. 4.

4 System Performance Demonstration

To measure the X-ray performance of the system, $\sim 10,000$ X-ray events per pixel are collected from the Fe-55 source installed on the snout's chimney, with a count rate of ~ 1.2 counts per second per pixel. The energy of the photons is estimated using the optimal filtering technique.²¹ To assess the spectral performance, the MnK α model²² is fitted to the collected, calibrated data. The model is convolved with a Gaussian broadening to parametrize the FWHM energy resolution

of the detectors. The goodness of the fit is estimated with the maximum likelihood method by means of a χ^2 statistics modified to mitigate biases due to bin size or number of events.²³

Each channel is activated by biasing the SSA, SQ1, and TES detectors at their optimal operating point. For the SSA, this is done by measuring its V - Φ curves for different bias currents and selecting the one with the largest modulation depth. The flux offset is chosen to operate the SSA on the steeper slope of its V_{out} versus Φ curve, both to minimize the system noise and to maximize the readout bandwidth. The same is repeated for the bias current of the SQ1s, selecting the one producing the maximum modulation depth. The flux offset of the SSA is then varied iteratively per row to find the value maximizing each SQ1's modulation depth. A voltage offset is then applied to center the FLL signal around zero to make optimal use of the feedback DAC dynamic range.

The TES bias is set to a value corresponding to roughly 17% of its normal resistance value, which during early measurements had shown to yield on average the best spectral performance, at the 150-nT magnetic field offset.

Measurements performed in this configuration showed a co-added energy resolution of 2.95 ± 0.03 eV. Implementing electrical crosstalk rejection in the analysis pipeline, based on known and understood crosstalk mechanisms in TDM systems,^{11,24} showed an improvement in the co-added performance. In particular, we applied time-neighbor and global cuts, as summarized in Fig. 8.

Time-neighbor cuts tag events that happen within a certain time window from an event happening in a subsequent or preceding row, whereas global cuts tag events happening within a time window regardless of their row number. In both cases, the cuts are limited to within the same column. To simplify the data analysis pipeline, we have applied here a crosstalk-rejection strategy that cuts all perpetrator-victim pairs within a readout column, with a time window of 2 ms. This strategy is suboptimal with respect to what is being envisaged for X-IFU so that the throughput of surviving counts in this dataset should not be understood as an analysis of what is possible for the flight pipeline of X-IFU. Furthermore, the impact of crosstalk on in-flight performance is expected to be lower than what is measured in the laboratory with the approximately monochromatic Fe-55 source, because the typical models assume a crab-like energy spectrum, with an average energy lower than 6 keV.^{11,25}

Experiments with a 1.2-cps count rate showed a larger impact on the co-added system performance. However, typical TDM laboratory demonstrations use a count rate at a level of 0.3 cps per pixel, similar to the expected average count rate for X-IFU when not observing high-intensity sources such as supernova remnants, gamma-ray burst afterglows or X-ray binaries in our galaxy.

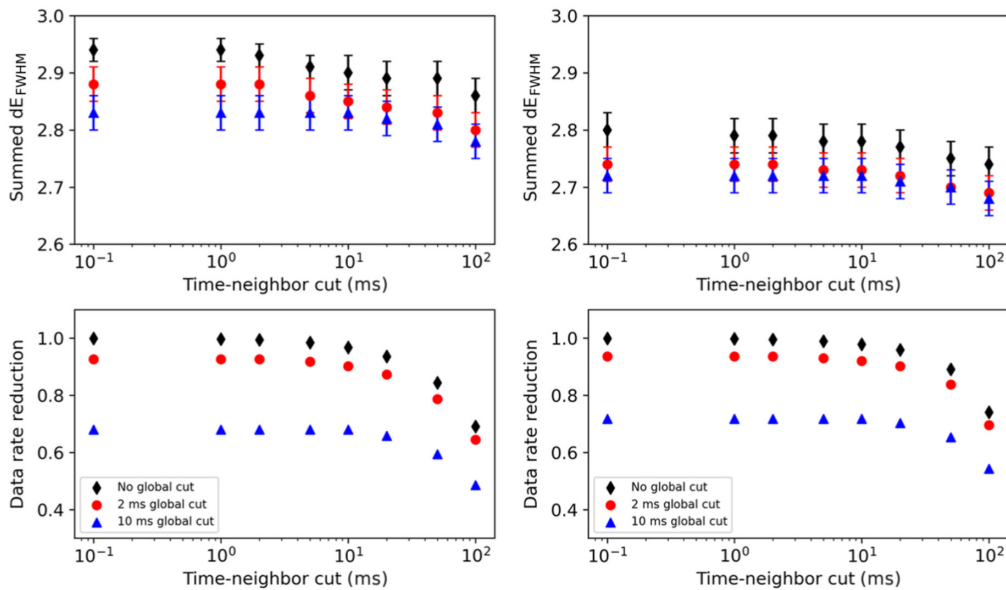


Fig. 8 Impact on the spectral performance of crosstalk rejection in the data analysis pipeline for the two count rates used.

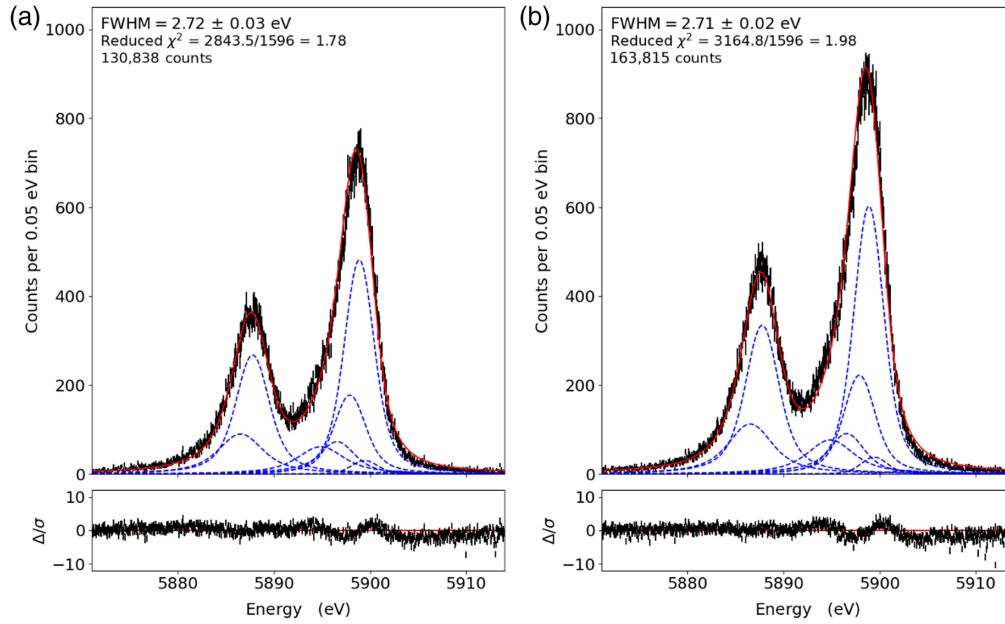


Fig. 9 Co-added spectra measured for the two columns of the system in 32-row readout: the histogram with the collected data in black, the best fit of the $\text{MnK}\alpha$ model convolved with a Gaussian broadening in red, and the individual spectral components of the model in dashed blue. The bottom panels show the residuals of the fit. In column 1, (a) five pixels were excluded from the analysis because of either malfunctioning components in the MUX or TES chip, or TESs receiving significantly fewer counts because of aperture mask misalignment. In column 2, (b) two pixels were excluded from the analysis, for the same reasons. The excess residual on the high-energy tail of the $\text{MnK}\alpha_1$ line is interpreted as due to the addition of spectra from pixels with different energy resolutions. (a) Column 1: 27 pixels co-added spectrum. (b) Column 2: 30 pixels co-added spectrum.

We therefore repeated the experiment by reducing the count rate to ~ 0.7 cps per pixel, by increasing the thickness of the Al foil in front of the cold ^{55}Fe source.

With the typical crosstalk cuts for laboratory TDM systems (20-ms window for time-neighbor and 2-ms window for global), we obtain a co-added performance of 2.72 ± 0.03 eV, with a data rate reduction of $\approx 8\%$ which already well fits the throughput requirements for X-IFU.² From this analysis, 5 of the 32 rows are excluded, due to either faulty cold components (TES or SQ1) or TES receiving significantly fewer counts because of aperture mask misalignment.

With the same configuration, we repeated the experiment for the second column of the setup. We measured consistent performance, with a co-added energy resolution of 2.71 ± 0.02 eV. For this column, 2 pixels were excluded from the analysis for the same reasons listed above.

The results for both columns are summarized in Fig. 9.

5 Conclusions and Future Outlook

We reported on the characterization of a cryogenic test bed to verify the performance of a TDM system with a long harness, toward the integration of the new focal plane assembly development model for X-IFU.

The re-designed flex harness allowed to mitigate the ringing observed in the previous version, at the cost of a reduced analog bandwidth. A bandwidth of ≈ 7 MHz was obtained by modifying the FB1 board in the analog electronics and choosing different settings for the ADC low pass filter in the DRE. In this way, it was possible to operate the system with a performance at the nominal level, with an energy resolution measured at a level of 2.7 eV at 5.9 keV energy.

This demonstration represents fundamental progress for the FPA-DM1.1 of X-IFU as it is the first time that a TDM system is operated with a 1.5-m-long harness, closer to the X-IFU's 2.3 m requirements.

NewAthena's instrument will employ twisted-pair looms in balanced differential operation, and so will the FPA-DM1.1. Having reached the expected level of performance for the system, in the near future, we will replace the current flex harness with twisted-pair looms to assess their impact not only on performance but also on crosstalk and analog bandwidth. This will be an important intermediate step before the integration and test campaign of the X-IFU FPA-DM1.1, foreseen for Q2 2025, which will allow us to assess the TDM readout operation in a configuration more representative of X-IFU. The comparison of the system behavior with a flex harness versus twisted-pair looms will be reported in a separate paper.

Disclosures

The authors declare there are no financial interests, commercial affiliations, or other potential conflicts of interest that have influenced the objectivity of this research or the writing of this paper.

Code and Data Availability

The corresponding author makes available the data presented in this paper upon reasonable request.

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Biographies of the authors are not available.